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# Lifetime Estimation of Grid-Connected Battery Storage and Power Electronics Inverter Providing Primary Frequency Regulation

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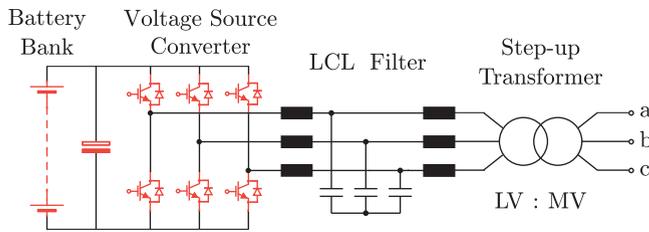
**ABSTRACT** Battery Energy Storage Systems (BESSs) are a new asset for Primary Frequency Regulation (PFR), an ancillary service for improving the grid stability. The system operators determine the implementation and remuneration of PFR. However, assessing the revenue stream is not enough to define the business case, as also the components' lifetime has to be estimated. Previous studies of lifetime estimation for BESSs performing PFR considered only the electrochemical storage, disregarding the power electronics (PE). Nonetheless, researchers have shown the importance of estimating PE wear due to the operation when applied in renewable energy generation and microgrids. This paper presents a lifetime analysis of BESSs providing PFR considering IGBT modules, electrolytic capacitors and electrochemical storage degradation. The lifetime information is used to estimate BESS's Net-Present-Value (NPV), evaluating the benefits of deploying PE-based BESS in the European grid. A comparison between different countries, Germany, the Netherlands, and the U.K., is performed, considering the PFR implementation and remuneration differences. The analysis shows that the BESS management strategy can extend its lifetime and that the component that exhibits the shortest lifetime is the electrochemical storage. The PE components are subject to low wear due to the low power utilization and, therefore, small thermal swings while performing PFR. In conclusion, the provision of PFR by means of BESS has been found to be profitable in all three countries. However, in the Netherlands, the potential NPV has been estimated to be 47% and 76% higher than in Germany and the U.K., respectively.

**INDEX TERMS** Battery energy storage system, lifetime estimation, net present value, primary frequency regulation, voltage source converter.

## I. INTRODUCTION

The rising of renewable energy-based generation plants is shifting the electrical energy production from large synchronous generators to Power Electronics (PE) interfaced distributed plants. Consequently, the inertia of the system and its regulating power, traditionally provided by large rotating synchronous generators, will likely decrease [1], [2]. System operators are then in need of finding new balancing resources. In this context, new assets are entering the grid balancing ancillary services, i.e., wind turbines [3], photovoltaic generators [4], and energy storage systems [5].

Battery Energy Storage Systems (BESSs), a technology characterized by high efficiency and relatively fast response [6], are particularly suitable for various balancing services, as grid inertial response [7], frequency nadir, and Rate of Change of Frequency (RoCoF) reduction [8], and Primary Frequency Regulation (PFR) [9]–[11]. PFR consists of varying the generator's power output proportionally to the fundamental frequency deviations from the nominal value, i.e., 50 Hz in Europe and China and 60 Hz in America. The technical implementation and remuneration of PFR in Europe are regulated by the national Transmission System Operators



**FIG. 1. Circuit schematic of a grid-connected BESS with the critical components in terms of lifetime highlighted in red.**

(TSOs), and it may differ between countries [12], [13]. BESSs are an emerging asset for PFR, also due to the clearly regulated remuneration, as opposed to other potential BESSs applications, i.e. voltage control, congestion management, peak shaving.

Although Lithium-ion BESSs show good technical suitability for PFR [14], [15], the high initial investment required to deploy such systems represents a barrier for system operators and private investors [16], [17]. Consequently, BESS's lifetime becomes a key factor for defining its business case.

Most high power commercial BESSs, e.g. from 100 kW to 5 MW, are based on a two-level Voltage Source Converter (VSC), constructed with three half-bridge legs for interfacing the battery bank with a Low Voltage (LV) AC grid [18]–[20]. Additionally, an LCL filter is used to contain the current harmonics injection inside the limits regulated by standards [21], and when needed, an auxiliary transformer is used to step up the voltage for the connection to the Medium Voltage (MV) grid. The described high power BESS system is shown in Fig. 1. Other elements, not shown in Fig. 1, exist for protection, such as AC and DC contractors, and electromagnetic compatibility filters.

Research in power electronic reliability shows that the main components within the VSCs subject to failure due to wear are the IGBT modules and the DC-link electrolytic capacitors [22]–[25]. Additionally, Lithium-ion based batteries have a limited lifetime, strongly influenced by the cycling pattern [26], and which generally spans from 3000 to 10000 cycles, depending on the lithium technology and the cycling conditions [27]. The IGBT modules, the electrolytic capacitors, and the electrochemical storage are then the components that are the most subject to wear in a BESS.

The degradation of IGBTs and electrolytic capacitors is mainly driven by the thermal stress to which they are subjected [28], [29], the electrochemical storage's degradation, instead, is mostly driven by its cycling pattern [26], [27]. In this respect, the lifetime of the battery cells providing PFR has been already investigated [15], nonetheless, in these studies the power electronic components have not been considered. Instead, prior research on PE converter lifetime has focused on other fields, such as wind [28] and solar generation [30], microgrids [29], STATCOM [31], and aerospace [32]. However, power electronic plays a significant role in BESSs, being the enabler technology used to interface the electrochemical storage with the AC grid. Above all, the PE wear constitutes

an important factor to be evaluated when studying BESS's lifetime [25].

This paper presents a mission profile based lifetime analysis of BESSs performing PFR as ancillary grid service. This grid service's choice is driven by the well defined technical, economic and regulatory framework of PFR, which allows the definition of a positive BESS's business case. The lifetime is defined by investigating the degradation of IGBT modules, electrolytic capacitors, and electrochemical storage. The components' lifetime models adopted, derived through accelerated lifetime testing, are taken from the manufacturers [33]–[35] and from the literature [36], [37]. Additionally, three case studies, particular to Germany, the United Kingdom (U.K.), and the Netherlands, with their differences in technical implementation and remuneration, are considered. To conclude, the economic viability of BESSs deployed to perform PFR is evaluated based on the information about components' replacement derived from the lifetime analysis.

The contribution of this paper is twofold: first, a mission profile based methodology to evaluate the lifetime of BESSs is proposed. The methodology is general; it can be used to estimate BESS's component lifetime for any BESS application, and, unlike other mission profile based BESS lifetime estimation methods proposed in literature [15], [17], it considers both electrochemical storage and power electronics wear. Second, technical and economic insights are presented after applying this methodology to a case study in which BESSs provide PFR in three European countries. More specifically, the lifetime information derived from analyzing electrochemical storage and PE wear is used to estimate BESS's Net-Present-Value (NPV). This allows evaluating the economic benefits of deploying PE-based BESS to provide ancillary services to the grid. The benefits are determined by comparing three case scenarios, reflecting three different energy markets in Europe, Germany, the Netherlands, and the U.K. The study considers the standardized PFR implementation, the BESS State-of-Charge (SoC) management, and remuneration schemes. This paper also highlights how BESSs' lifetime and business case are influenced by the existing differences between the countries where the technology is applied.

## II. PRIMARY FREQUENCY REGULATION MARKET

Primary frequency regulation is an ancillary service typically offered by generators connected to the transmission networks. This service may assume different names depending on the country, however, in the remainder of the paper, it will be referred to as PFR. PFR is a process to maintain stability in the power system by reacting to frequency variations. When a frequency change  $\Delta f$  occurs after a fluctuation in the generation or load, the PFR operates to adjust the active power output of the generators and other available controllable units in the system, such as BESSs. The power output is adjusted according to a droop characteristic that follows  $\Delta f$ . An example of such droop control logic is shown in Fig. 2. Both the U.K. and Germany adopt a deadband, which is a frequency interval around the nominal value in which the system is not required

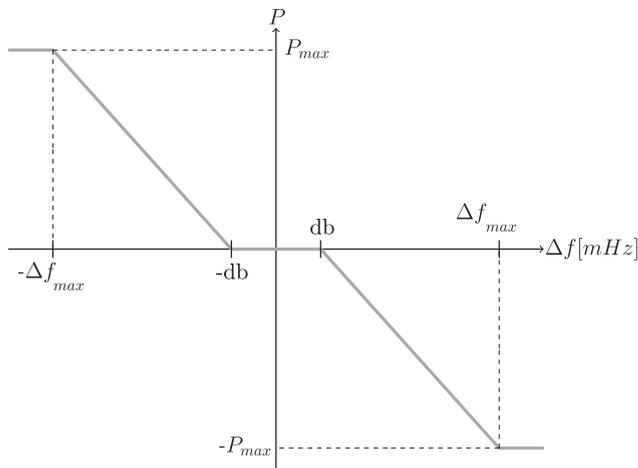


FIG. 2. Example of a P-f droop control curve for PFR provision.

to exchange power with the grid. This deadband has a different amplitude for U.K. [38] and Germany [39], i.e.  $\pm 15$  mHz and  $\pm 10$  mHz respectively [12]. In the Netherlands, an insensitivity range of  $\pm 10$  mHz is implemented instead [40]. The insensitivity range acts as a moving deadband, requiring the unit to change its power output only if a frequency variation greater than 10 mHz from the current operating point is detected [40]. Despite the differences in the deadband and insensitivity range, in all three countries the maximum regulating power has to be delivered for frequency variations higher than a preset threshold, i.e., 200 mHz in Germany [39] and the Netherlands [40], and 500 mHz in the U.K. [38]. Additionally, energy limited resources, such as BESSs, are required to be able to keep the maximum power for frequency variations  $\geq 200$  mHz for at least 15 or 30 minutes. The minimum required power of generators and BESSs providing such service is generally  $> 1$  MW. However, owners of multiple sources of low power grid assets, such as stationary batteries, industrial processes, renewable energy generation, and Electric Vehicles (EVs) charging stations, can cluster their power capability together to deliver the minimum required power [10], [38]–[40].

To participate in the PFR market, Balance Service Providers (BSPs) submit their bids to the responsible TSO. The bids are composed of the available regulating power and the required price for activation. Each TSO defines how much regulating power must be available in their control area at each instant; with this information they set up the tenders. After collecting all BSPs's bids, the cheapest feasible bids (that guarantee the required regulating power in the area) are selected.

The frequency trend of continental Europe [39] and the U.K. [42] during the year 2018 are plotted in Fig. 3. From this figure, it is possible to see that in the U.K., the grid frequency is subject to wider variations than in continental Europe; this is due to the lower inertia of the system. By following the frequency oscillations, energy limited resources, such as BESSs, will inevitably see a deviation of their SoC. Then, to ensure the system's continuous availability in providing PFR, the SoC

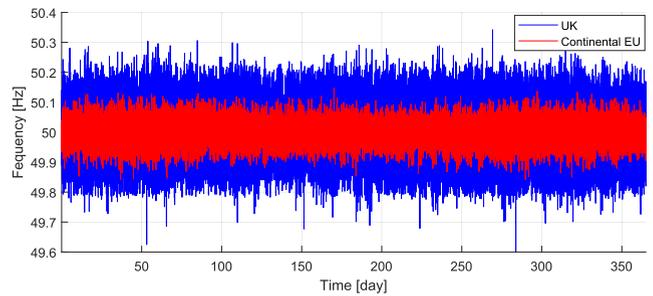


FIG. 3. Measured frequency trend in U.K. [38] and continental Europe [41] during 2018.

of the battery has to be controlled. In this context, a fraction of the BESS power can be reserved for managing the SoC and for keeping it close to a reference value. Consequently, the frequency regulation service is provided only with the remaining available power. Alternatively, when the deadband is contemplated in the droop function, the SoC control can be done when the frequency variations are inside the deadband, and so the output power of the system for PFR should be zero. Nonetheless, a recent guidance published by National Grid, the system operator of the U.K., recommends that BESSs should withhold a fraction of the power for the SoC management, and not use the deadband for regulating the SoC [43]. For these reasons, in the remainder of the paper, only the SoC management strategy through the withholding of a fraction of the full system power will be considered. Therefore, the sum of the maximum power for SoC management  $P_{\text{SoC,max}}$  and for the frequency regulation  $P_{\text{pfr,max}}$  is always equal to the maximum system power,  $P_{\text{tot}}$ :

$$P_{\text{tot}} = P_{\text{SoC,max}} + P_{\text{pfr,max}}. \quad (1)$$

As previously mentioned, the payment for PFR is proportional to the power tendered. Then, withholding a fraction of the total power for managing the SoC would inherently reduce the frequency regulation market revenues. However, the system's power utilisation would reduce, and so it would advantageously extend the lifetime of the BESS. The algorithm for the provision of PFR is illustrated in Fig. 4. The SoC regulation occurs in parallel to the PFR provision, targeting the re-establishing of the SoC at 50%, so that the BESS is able to deliver symmetrically for long time both up and down regulation, with the maximum energy available, in case of a strong frequency perturbation [14], [15]. Other parallel SoC re-establishing strategies could be implemented, for example containing the SoC into a range of values, however, these are not considered in this study.

### III. BATTERY ENERGY STORAGE SYSTEM DESIGN

In this study, a BESS rated 150 kW/150 kWh has been considered, assuming that the BESS is aggregated with other BSPs to reach the minimum required power for PFR, i.e., clustering together up to 1 MW for PFR.

The VSC circuit topology consists of three half-bridge IGBT-Diode modules. A Low Voltage (LV) DC-link is taken

TABLE I BESS Design Specifications and Components Selection

Design Parameter	Value	Components selected		
Rated VSC power	$S_n$	150kVA	IGBT modules	Infineon FF300R12KE4
DC link voltage	$V_{dc,n}$	750 - 1000V	Electrolytic Capacitors	Cornell Dubilier Type 500C
AC line-to-line voltage	$V_{ac,ll}$	400 V	Battery technology	LiFePO <sub>4</sub>
Switching frequency	$f_s$	12 kHz	Heat Sink	From Infineon inverter stack 6PS0300R12KE3

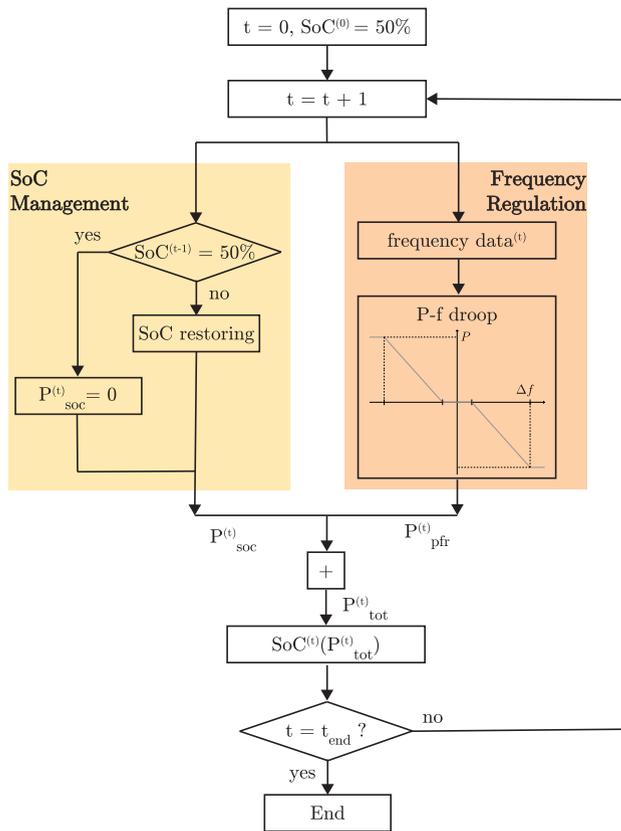


FIG. 4. Flowchart describing the algorithm for PFR provision, where  $t$  indicates the time instant and  $P_{pfr}^t$  and  $P_{soc}^t$  are respectively the frequency regulation power and the SoC control power at the instant  $t$ .

into account,  $V_{dc} = 750\text{--}1000$  V, coherently with the specifications of commercial battery racks [44], [45], and so for the connection at the Medium Voltage (MV) network, a LV/MV transformer is necessary to step up the voltage from the 400 V line-to-line output of the VSC. The BESS' circuit schematic is shown in Fig. 1 and the three components of which the lifetime is investigated, the electrochemical storage, the IGBT modules, and the electrolytic capacitors installed in the DC-link, are highlighted in red. The design specifications and the components selected, according to the procedure described in the following, are summarized in Table I, where  $S_n$  stands for the rated VSC power,  $V_{dc}$  and  $V_{ac,ll}$  for DC link and AC line-to-line voltages and  $f_s$  for the VSC's operating switching frequency.

The commercially available Trench/Fieldstop IGBT4-Diode modules FF300R12KE4, capable of withstanding up to 300 A at junction and case temperatures of respectively 175 °C and 100 °C and of the 1200 V voltage class, are selected [46]. These IGBT modules are selected based on the DC voltage, the peak collector current they have to carry and to ensure that the three VSC's legs deliver an efficiency greater or equal to 97.5% at the rated power of 150 kVA. The IGBT modules of a VSC are subject to power losses due to the current conduction and hard switching. The semiconductors' losses cause thermal stress in its chips and module package constituents, which drives their degradation [34]. The conduction losses  $P_c$  and the switching losses  $P_s$  for a Sinusoidal Pulse Width Modulation (SPWM) controlled VSC can be analytically calculated as function of the modulation index  $M$ , the switching frequency  $f_s$ , equal to 12 kHz in this study, the peak AC current  $\hat{I}_{ac}$ , and the phase shift angle between the output AC voltage and current  $\varphi$ , through (2)–(3) for the IGBTs and (4)–(5) for the diodes [34].

$$P_{c,T} = \left( \frac{1}{2\pi} + \frac{M \cos \varphi}{8} \right) [v_{ce,25} + tc_{vt} (T_j - 25)] \hat{I}_{ac} + \left( \frac{1}{8} + \frac{M \cos \varphi}{3\pi} \right) [r_{ce,25} + tc_{rt} (T_j - 25)] \hat{I}_{ac}^2 \quad (2)$$

$$P_{s,T} = \frac{f_s E_{on+off} \hat{I}_{ac}}{\pi 300} [1 + a_t (T_j - 25)] \left( \frac{V_{dc}}{600} \right)^{k_{vt}} \quad (3)$$

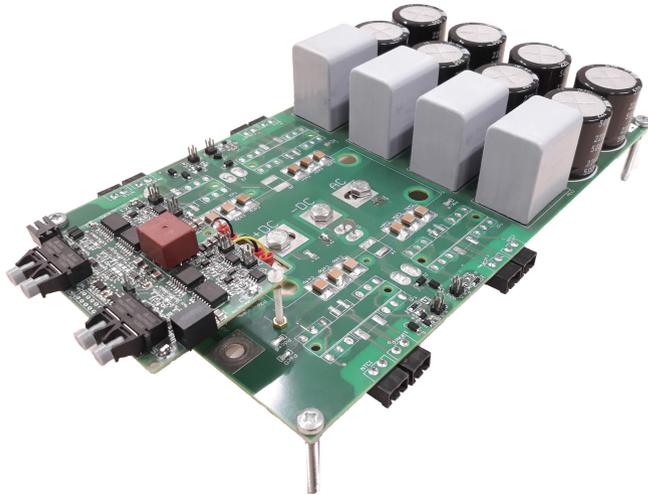
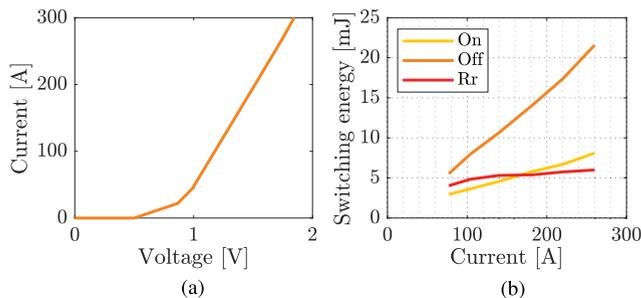
$$P_{c,D} = \left( \frac{1}{2\pi} - \frac{M \cos \varphi}{8} \right) [v_{f,25} + tc_{vd} (T_j - 25)] \hat{I}_{ac} + \left( \frac{1}{8} - \frac{M \cos \varphi}{3\pi} \right) [r_{f,25} + tc_{rd} (T_j - 25)] \hat{I}_{ac}^2 \quad (4)$$

$$P_{s,D} = \frac{f_s E_{rr} \sqrt{2}}{\pi} [1 + a_d (T_j - 25)] \left( \frac{\hat{I}_{ac}}{300} \right)^{k_i} \left( \frac{V_{dc}}{600} \right)^{k_{vd}} \quad (5)$$

where  $V_{ce,25}$ ,  $r_{ce,25}$ ,  $v_{f,25}$ ,  $r_{f,25}$  are the coefficients modeling the on-state losses of IGBTs and diodes at 25 °C. The on-state parameters are temperature dependent, as expressed in (2) and (4), following the coefficients  $tc_{vt}$ ,  $tc_{rt}$ ,  $tc_{vd}$ , and  $tc_{rd}$  whose value is summarized in Table II.  $E_{on+off}$  and  $E_{rr}$  are the hard switching added turn-on and turn-off energy losses, and reverse recovery energy losses, respectively, derived for a switched voltage  $V_{dc}$  and current of 600 V and 300 A, junction temperature of 25 °C and external gate resistance of 2Ω.  $k_{vt}$ ,  $k_i$ ,  $k_{vd}$ ,  $a_t$ , and  $a_d$  are scaling coefficients for the switching energy taken from [34]. The test board shown in Fig. 5 is used

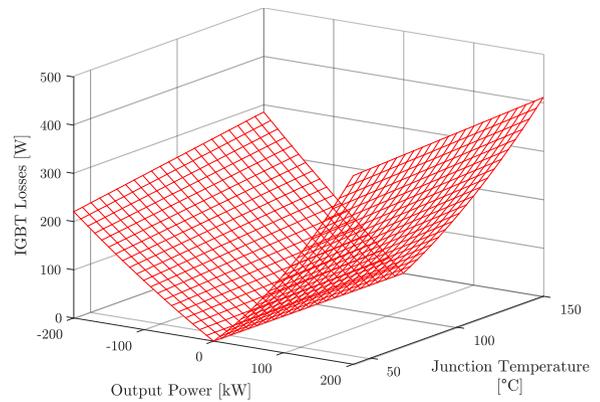
**TABLE II** Parameters for Estimating Power Losses of the IGBT Module FF300R12KE4 [34]

IGBT		Diode	
Parameter	Value	Parameter	Value
$v_{ce,25}$	0.9 V	$v_{f,25}$	1.05 V
$r_{ce,25}$	2.7 m $\Omega$	$r_{f,25}$	1.9 m $\Omega$
$t_{Cvt}$	-0.0011	$t_{Cvd}$	-0.0022
$t_{Crt}$	$1.28 \cdot 10^{-5}$	$t_{Crd}$	$7.2 \cdot 10^{-6}$
$E_{on+off}$	39 mJ	$E_{rr}$	6 mJ
$a_t$	0.003	$a_d$	0.006
$k_{vt}$	1.35	$k_{vd}$	0.6
		$k_i$	0.6


**FIG. 5.** Test board for the characterization of semiconductor modules and/or TO-packaged discrete devices.

**FIG. 6.** Conduction (a) and switching at  $V_{dc} = 600$  V (b) characteristic of the IGBT-Diode modules FF300R12KE4 measured through the test board of Fig. 5 with junction temperature of 25 °C and external gate resistance of 2 $\Omega$ .

to derive the on-state and switching characteristics, plotted in Fig. 6. Table II summarizes the coefficients and parameters used in (2)–(5) for the semiconductors losses calculations.

Loss-maps are used for the junction temperature estimation for a given mission profile, so to speed up the computation. These relate the power losses in the IGBTs and Diode to the junction temperature and converter output power and are generated through (2)–(5). An example of the IGBT loss-map is shown in Fig. 7, where the losses in an IGBT are shown as function of its junction temperature and of the VSC output power.


**FIG. 7.** Loss-map of a single IGBT of the Trench/Fieldstop IGBT4-Diode modules FF300R12KE4 as function of its junction temperature and of the SPWM modulated at 12 kHz VSC's output power, for a DC link voltage of 900 V and an AC line-to-line voltage of 400 V.

Another component of the VSC of interest from the lifetime point of view is the electrolytic capacitor bank placed between the electrochemical storage and the IGBT modules in the DC-link. The DC-link capacitors function both as an energy buffer and limit the DC voltage ripple. To ensure a safe and efficient DC-AC power conversion, without over modulating the PWM controlled VSC, it is required that half the DC voltage is always higher than the maximum peak AC voltage  $\hat{V}_{ac,max}$  [47]:

$$\frac{V_{dc,min}}{2} - \frac{\Delta V_{dc,r}}{2} \geq \hat{V}_{ac,max}, \quad (6)$$

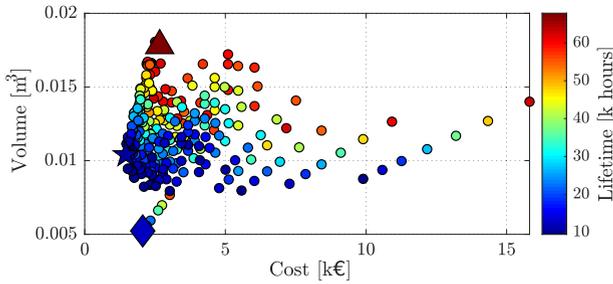
where  $V_{dc,min}$  is the minimum battery DC voltage and  $\Delta V_{dc,r}$  is the DC voltage ripple. In this respect, the battery's open-circuit voltage variations due to the SoC, and the international grid codes, that require the normal operation for  $\pm 10\%$  voltage deviation from the nominal value play a crucial role. As discussed in [48], the DC-link voltage ripple  $\Delta V_{dc,r}$ , for SPWM modulation strategy, symmetrical grid, and balanced load, is composed of only the high frequency components, and it can be expressed as:

$$\Delta V_{dc,r} = \frac{3 M \hat{I}_{ac} \cos \varphi}{8 f_s C_{dc,r}} (1 + M), \quad (7)$$

where  $C_{dc,r}$  is the DC-link capacitance value. However, in the case of unbalanced fundamental frequency loading, a second harmonic component in the DC voltage ripple arises [48]. In this case, the low-frequency component dominates the high-frequency one, and so the DC ripple takes the following expression [48]:

$$\Delta V_{dc,r} = \frac{3 M \hat{I}_{-}}{8 \pi f_g C_{dc,r}}, \quad (8)$$

where  $\hat{I}_{-}$  is the peak value of the negative sequence current and  $f_g$  is the grid nominal frequency of 50 Hz. Equation (8) considers a three wire system, so that no zero sequence component is present. However, in this study, the balanced operation of the converter is considered and so the minimum



**FIG. 8.** Volume, costs and lifetime of the DC-link capacitor designs that meet the design, thermal and base lifetime requirements. The star indicates the solution with the minimum cost, the diamond the one with minimum volume, and the triangle the one with maximum base lifetime.

capacitance value  $C_{dc,r}$  that satisfy the DC-link voltage ripple constraint can be found combining (6) and (7).

Concerning the energy buffer functionality of the DC-link capacitors, these are sized to be able to sustain a load step of  $\Delta P$ , in a period of  $T_r$ , allowing a voltage deviation of  $\Delta V_{dc}$  [49]:

$$C_{dc,e} \geq \frac{T_r \cdot \Delta P}{(2 \cdot V_{dc} \Delta V_{dc})}. \quad (9)$$

$T_r$  depends on the DC-AC converter control delay, and it is usually selected as 5 to 10 modulation periods.

The DC-link capacitance  $C_{dc}$  can be selected as the largest value between  $C_{dc,r}$  and  $C_{dc,e}$  that are the minimum capacitance values that ensure the fulfillment of the voltage ripple and energy buffer design requirements, derived through (6)–(9):

$$C_{dc} \geq \max \{C_{dc,e}, C_{dc,r}\}. \quad (10)$$

Additionally, the DC-link capacitors have to withstand the current flowing through them, that can be analytically calculated for the symmetric system as [50]:

$$I_{dcl} = \hat{i}_{ac} \sqrt{M \left[ \frac{\sqrt{3}}{4\pi} + \left( \frac{\sqrt{3}}{\pi} - \frac{9}{16}M \right) \cos^2 \varphi \right]}. \quad (11)$$

In this study, several commercially available capacitors of the  $500V_{dc}$  class from [51] have been considered. Given the maximum value of  $I_{dcl}$  and the current capability of the single capacitors, the number of parallel capacitor strings, which consists of two series capacitors, are found. In this way, according to the components' characteristics, several DC-link designs are derived. The solutions that do not satisfy the minimum capacitance constraints given in (10) or that show a maximum hot-spot temperature higher than  $95^\circ\text{C}$ , the limit set in the data-sheet, are discarded. The volume, costs and base lifetime that stands for the number of guaranteed hours operating at  $85^\circ\text{C}$ , and maximum allowed ripple current of the remaining designs are plotted in Fig. 8. These designs respect quality and performance constraints. For further analysis, the design that offers the least cost is selected, where the commercial cost figures are derived from [52]. This is done because market competitive industrial products are often

designed, targeting the minimization of costs. Moreover, since grid-connected BESS are generally deployed in containers, volume minimization is not a driver as strong as cost minimization. Additionally, in terms of power losses, any substantial gain in efficiency by reducing capacitor losses would lead to prohibitive cost figures because the electrolytic capacitors' losses are relatively much smaller than the ones seen in the semiconductors. Therefore, the design with the lowest cost that guarantees the quality and performance required, indicated with a star in Fig. 8, is selected. This DC-link configuration consists of six parallel strings of two series connected capacitors of 3.9 mF.

#### IV. BATTERY ENERGY STORAGE SYSTEM LIFETIME MODEL

In this Section, the lifetime models for the electrochemical storage, the IGBT modules and the electrolytic capacitors are discussed.

##### A. ELECTROCHEMICAL STORAGE LIFETIME

Lithium-ion batteries are subject to several ageing mechanisms. This causes an increase in the cell's impedance and the decrease of cyclable lithium [27], [53]. Such conditions lead to a lower battery's energy capacity, power capability, and round trip efficiency [54]. In this respect, it is common practice to consider a capacity fading of 20% as a reference value for the End of Life (EoL) of grid-connected BESS and EV battery packs.

Research has shown that both the power cycling and the idling condition contribute to the ageing of Li-ion based batteries. In this study, to evaluate the electrochemical cells lifetime, the empirical model for  $\text{LiFePO}_4$  batteries developed through accelerated cycling of battery cells [36] and proposed in [37] is adopted. This model has been already adopted for the estimation of battery degradation in PFR [15], [55] and wind power applications [36], [37]. The capacity fading due to calendar ageing,  $C_{cal}$ , and cycling ageing,  $C_{cyc}$ , in percentage, are then evaluated according to (12) and (13) respectively [37]:

$$C_{cal} = 0.1723 \cdot e^{0.007388 \cdot SoC_1} \cdot t^{0.8} \quad (12)$$

$$C_{cyc} = 0.021 \cdot e^{-0.01943 \cdot SoC_{avg}} \cdot cd^{0.7612} \cdot nc^{0.5}. \quad (13)$$

The capacity fading is then a function of the average SoC of a cycle  $SoC_{avg}$ , the number of cycles  $nc$  of a certain cycle depth  $cd$ , and the idling time  $t$  of the battery at a certain SoC level  $SoC_1$ . Equations (12) and (13), which describe the capacity fading, are derived for a Lithium-ion battery at a temperature of  $25^\circ\text{C}$ . However, temperature strongly influences Lithium-ion batteries' ageing [37], yet, grid-connected BESSs are generally deployed in containers equipped with air conditioning systems, used to control the temperature of the battery cells. Mostly, the temperature is kept stable at  $25^\circ\text{C}$ , to ensure optimal performances and extend its lifetime [55].

**TABLE III** Foster Thermal Model Parameters of IGBTs, Diodes and Heatsink Used for the study [46], [59]

i	IGBT		Diode		Heatsink	
	R [K/W]	$\tau$ [s]	R [K/W]	$\tau$ [s]	R [K/W]	$\tau$ [s]
1	0.00558	0.01	0.009	0.01	0.01374	2.23
2	0.03069	0.02	0.0495	0.02	0.04543	51.334
3	0.02976	0.05	0.048	0.05	0.0006	88.93
4	0.02697	0.1	0.0435	0.1	0.01573	88.93

## B. SEMICONDUCTOR LIFETIME

Power semiconductors and their packaging are subject to several failure mechanisms, such as bond wire lifting and breakage, and solder plate fatigue on the base plate and in the chip soldering [56]. Among these, bond wire related failures are the most prominent cause of power modules failures [57]. These are caused by the thermo-mechanical stress induced by the temperature gradients between the components due to the different materials and power losses [34]. In this context, research is focused on online junction temperature estimation methods, so to optimize the power module operation to enhance its reliability [58].

To evaluate the junction temperature of the semiconductors, the thermal behaviour of the semiconductor and the cooling aggregate is modelled through the Foster parameters as given by the manufacturer's datasheet [46], [59]. The forced air cooling aggregate implemented in the Infineon inverter stack 6PS0300R12KE3 has been taken as reference [59]. Its Foster parameters,  $R_i$  and  $\tau_i$ , used to represent the thermal behaviour of the power modules, together with the one of IGBTs and diodes, are listed in Table III. This heatsink has been chosen to guarantee that when the VSC operates at maximum power the steady-state junction temperature does not exceed 140 °C, leaving a safe margin from 150 °C, which is the maximum allowed temperature during switching conditions according to the IGBT modules' data-sheet [46].

The number of cycle to failure  $N_f$  of an IGBT module subject to a thermal cycle of amplitude  $\Delta T_j$ , minimum junction temperature  $T_{j,\min}$ , and with heating time  $t_{\text{on}}$  are estimated through:

$$N_f = A \cdot \Delta T_j^{\beta_1} \cdot e^{\frac{\beta_2}{T_j + 273}} \cdot t_{\text{on}}^{\beta_3} \cdot I_B^{\beta_4} \cdot V_C^{\beta_5} \cdot D^{\beta_6}. \quad (14)$$

Equation (14) is resulting from several empirical studies, based on power cycling of multiple IGBT modules [33], [34]. The number of cycles to failure are determined also as function of the current per bond wire  $I_B$ , the module voltage class  $V_C$ , the bond wire diameter  $D$ . The coefficient  $A$  relates to the IGBT technology and it is equal to  $9.34 \cdot 10^{-4}$  for Infineon IGBT4, while  $\beta_1 \dots \beta_7$  are selected according to [34]. Further experimental studies have updated (14), showing how semiconductor degradation saturates with thermal cycles with load periods ( $t_{\text{on}}$ ) longer than 60s [29], [60]. Then, the influence of the loading time, when longer than 60 s, can be modelled in (14):

$$\frac{N_f(t_{\text{on}})}{N_f(1.5)} = 0.33, \quad t_{\text{on}} \geq 60\text{s}. \quad (15)$$

The IGBT module's consumed lifetime due to a specific cycle  $p$  is found as the reciprocal of  $N_{f,p}(\Delta T_{j,p}, T_{j,p}, t_{\text{on},p})$ . When the consumed lifetime reaches the unity the module is considered at the end of life. Hence, the semiconductor lifetime can be estimated as:

$$L_s = \frac{1}{\sum_{p=1}^N CL_{s,p}} = \frac{1}{\sum_{p=1}^N \frac{n_p}{N_{f,p}}}, \quad (16)$$

where the index  $p = 1 \dots N$  represents the distinct thermal cycles and  $n_p$  the occurrences of the cycle  $p$  during a certain period of time.

## C. ELECTROLYTIC CAPACITOR LIFETIME

The electrolytic capacitors' degradation mainly depends on two factors, operating voltage and the hot-spot temperature [22], [61]. Manufacturers often give lifetime models of aluminium electrolytic capacitors, and in this study, it is modelled as [35]:

$$L_c = L_b \cdot \left(4.3 - 3.3 \frac{V_a}{V_r}\right) \cdot 2^{\frac{T_m - T_c}{10}} \quad (17)$$

where  $L_b$  is the rated capacitor lifetime,  $V_a$  is the applied voltage and  $V_r$  is rated voltage,  $T_m$  is the maximum rated core temperature, and  $T_c$  the operating core temperature [35].  $T_m$  and  $L_b$  are related to the capacitor packaging and manufacturing, as specified by the manufacturer [35]. The operating hot-spot temperature,  $T_c$ , is estimated based on the capacitor Equivalent Series Resistance (ESR), the thermal resistance  $Z_{\text{th}}$ , both from data-sheet, and on the current flowing through the capacitor. In this regard, the full harmonic spectrum of the DC-link current,  $I_{\text{cap},h}$ , and the ESR<sub>*h*</sub> variation according to the current harmonic frequency  $h$  have to be considered [35]:

$$T_c = T_a + 1.5 \cdot Z_{\text{th}} \cdot \left( \sum_{h=1}^{\infty} I_{\text{cap},h}^2 \cdot \text{ESR}_h + I_{\text{leak}}(V_{\text{op}}) \cdot V_{\text{op}} \right), \quad (18)$$

where  $I_{\text{leak}}$  is the capacitor leakage current as function of  $V_{\text{op}}$ , given by the datasheet and  $V_{\text{op}}$  the operating voltage [51]. When (18) is adopted for lifetime estimation purposes, the capacitor manufacturer recommends the introduction of the coefficient 1.5, so that the heat rise due to current ripple weights more than the ambient temperature  $T_a$  effect [35].

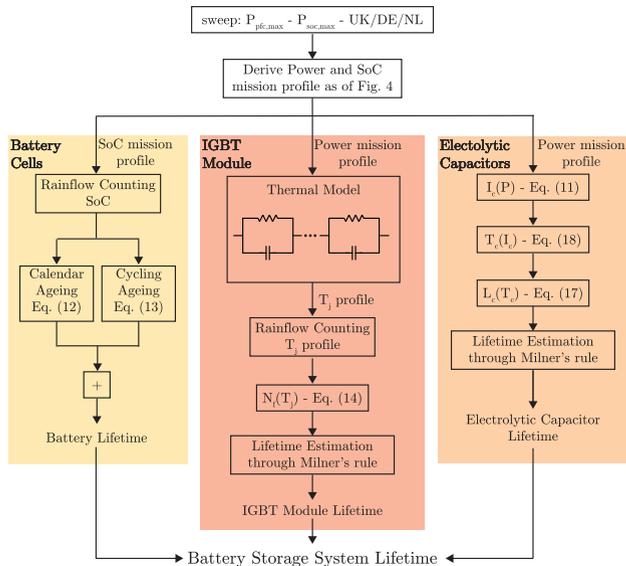
Given the hot-spot temperature profile, the accumulated damage can be determined through Miner's rule [62]:

$$CL_c = \sum_{i=1}^K \frac{t_i}{L_{c,i}}, \quad (19)$$

where  $t_i$  is the time during which the capacitor is operating in a specific condition  $i$  and  $L_{c,i}$  is the lifetime at this operating condition.

## V. LIFETIME EVALUATION METHODOLOGY

The procedure adopted for evaluating the BESS lifetime is illustrated in Fig. 9. Such methodology has the peculiarity of considering not only the degradation of the electrochemical

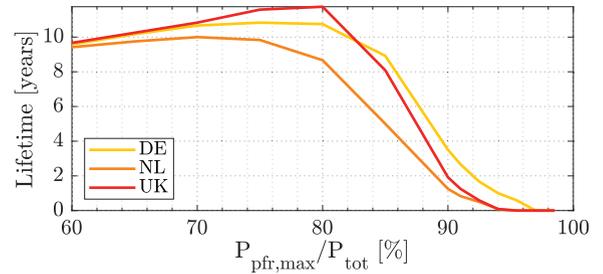


**FIG. 9.** Methodology used for the lifetime estimation of electrochemical storage, semiconductor modules, and electrolytic capacitors.

storage, left part of Fig. 9, as proposed in literature [15], [17], but also the IGBT module and electrolytic capacitor one, centre and right parts of Fig. 9.

Starting from the droop logic and the frequency trends, shown respectively in Fig. 2 and Fig. 3, the output power of the BESS is calculated. The algorithm for PFR provision is illustrated in Fig. 4. As discussed in Section II, this procedure is repeated varying the power sharing between PFR  $P_{pfr,max}$  and SoC management  $P_{soc,max}$ , respecting (1). Therefore, starting from the frequency trend, one year power and SoC mission profiles are defined, as detailed in Section II. The SoC profiles are then decomposed between idling time when the battery system is not exchanging power with the grid and cycling time. The idling time and SoC levels are substituted in (12) to estimate the yearly calendar degradation. A rainflow counting algorithm is applied to the cycling profile, and so the equivalent cycles performed by the battery during the year are found [63]. These are substituted in (13) to determine the battery's capacity fading due to power cycling. The yearly capacity fading is derived by adding the contribution of calendar and cycling ageing. Finally, the storage lifetime is obtained by estimating when the capacity fading reaches 20% and thus, its EoL.

The output power found through the algorithm shown in Fig. 4 is the main input for the lifetime estimation of the IGBT modules junction temperature and of the electrolytic capacitors. At the first iteration, the IGBT module junction temperature is considered 40 °C, the air cooling system's reference temperature. For each following iteration, given the semiconductors junction temperatures and the converter output power, the IGBT and diode losses can be estimated through the loss-maps generated with (2)–(5), of which an example is shown in Fig. 7. Once derived the semiconductor power losses, the heatsink's temperature, power module case,



**FIG. 10.** Battery cells' lifetime varying the percentage of the total power used for PFR provision,  $P_{pfr,max}$  in the case scenarios of Germany, the Netherlands and the U.K.

and chip die junctions can be updated through the Foster thermal model.

Once the last iteration is reached and the thermal profile of the semiconductors junction is derived, this can be decomposed in equivalent thermal cycles through a rainflow counting algorithm [63]. Number of cycles to failure,  $N_{f,p}$ , for the specific cycles are calculated through (14). Then, the consumed lifetime of the power module  $CL_{s,year}$  is estimated summing the contribution of each cycle  $p$ ,  $CL_{s,year} = \sum_{p=1}^N CL_{s,p}$ , and its lifetime through the reciprocal of the yearly consumed lifetime:

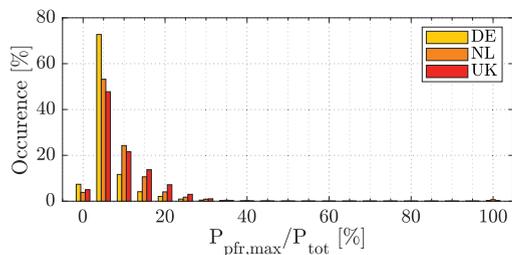
$$L_s = \frac{1}{\sum_{p=1}^N CL_{s,p}}. \quad (20)$$

Regarding the electrolytic capacitor lifetime estimation, the capacitors current  $I_{dcl}$  can be estimated through (11) and starting from the output power and SoC mission profile. Then, the current flowing in each capacitor is found dividing  $I_{dcl}$  with the number of parallel capacitors strings. The current profile through the capacitors gives the hot-spot temperature profile that, implemented in (19), gives the capacitor wear due to the operation. Following a similar procedure to the one of the IGBT modules, the capacitor lifetime is calculated as the reciprocal of its consumed lifetime  $CL_c$ , as described in Section IV.

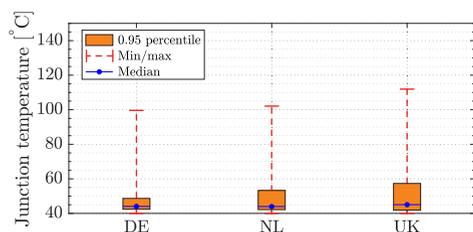
## A. RESULTS AND DISCUSSION

The BESS mission profile is generated varying fraction of power assigned to PFR  $P_{pfr,max}$  and the one assigned to the SoC management  $P_{soc,max}$  following the algorithm described in Section II.

Running the procedure detailed in Section V and Fig. 9, the electrochemical storage lifetime is estimated, and shown in Fig. 10. The results show that reducing the power reserved for PFR,  $P_{pfr,max}$ , the battery bank lifetime can be extended, reaching the peak at around  $P_{pfr,max}$  equal to 70%-80%  $P_{tot}$ . However, by doing so, the revenues would decrease since the payment scheme depends on the power bid in the tenders,  $P_{pfr,max}$ , as the following section will discuss. The lifetime of the IGBT modules of the VSC is dependent on the junction temperature profile. These IGBT and Diode temperature profiles are estimated following the methodology detailed in Section IV-B and in Fig. 9.



**FIG. 11.** Time distribution of the BESS output power for PFR provision operating with  $P_{\text{pfr,max}} = 150$  kW in the case scenarios of Germany, the Netherlands and the U.K.

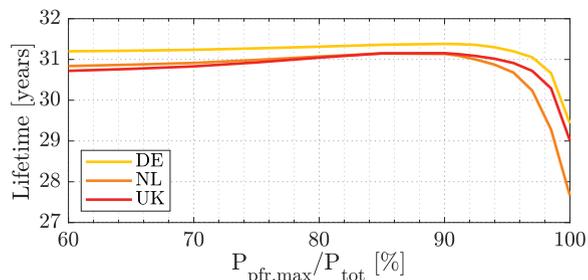


**FIG. 12.** Estimated junction temperature analysis of the BESS's IGBTs providing PFR in the case scenarios of Germany, the Netherlands and the U.K.

As shown in Fig. 11 analyzing the BESS power mission profile for  $P_{\text{pfr,max}} = 150$  kW, it can be seen that around 95% of the time during the year the system operates at a very low partial load,  $\leq 20\%$  of the total rated output power. This results from the nature of the P-f droop curves and the usually low frequency variations observed in the network. Therefore, this functionality's very low power utilization inevitably leads the VSC to operate at low junction temperature and only seldom reach the thermal limits. Working at low temperature and seeing small power output variations, the IGBT and diode junction is subject to low thermal stress when applied for this specific application. In Fig. 12, the estimated IGBT junction temperature average value and the 0.95 percentile over the yearly load profile are shown, and they can be seen to be very low. However, the derating of the cooling aggregate or of the semiconductor for reducing system costs is not a feasible option, since the BESS has to be capable to deliver the full power and as can be seen in Fig. 12 the IGBTs' junction can reach high temperature values, although sporadically.

Such low thermal stress, as expressed in (14) and so by the manufacturer [33], [34], leads to low semiconductor degradation. Therefore, for BESS VSC performing PFR, the IGBT modules are not strongly subject to degradation due to the normal operation. Other causes of failure, related, for example, to the environmental conditions or grid transients, however, remain [23].

The electrolytic capacitors also encounter a similar lifetime trend to the one shown by the electrochemical storage and the IGBT modules. As it is possible to see in Fig. 13, the reduction of  $P_{\text{pfr,max}}$  leads to an increase of the lifetime. Nonetheless, the lifetime extension is less pronounced than the one seen by the electrochemical storage.



**FIG. 13.** Electrolytic capacitor lifetime varying the percentage of the total power used for the provision of frequency regulation in the case scenarios of Germany, the Netherlands and the U.K.

## VI. ECONOMIC ANALYSIS

The market for Lithium-ion batteries is rapidly growing due to increased demand for electric vehicles and stationary storage applications, reporting a 75% decrease in battery pack's price from 2013 to 2019 [5], [65], [66]. For this study, the capital cost of electrochemical storage has been considered 330 €/kWh, according to the latest published report by the US National Renewable Energy Laboratory [67]. The operation and maintenance (O&M) cost are set to 4.5€/kWh/year [17]. The cost for the Power Electronics Converter (PEC) and the Balance of the Plant (BoP) has been derived according to the solar utility market, since utility scale VSCs of photovoltaic generators are similar systems to the ones used in BESS, and fixed to 150€/kW [68], [69].

The remuneration scheme for the PFR provision in the selected countries foresees a payment to the service provider proportional to the regulating power and to the time of provision accepted in the tender, the price is then specified as €/MW/h. Germany fully contracts its regulating power through a joint auction between several central European countries. The Netherlands participates in the joint auction as well; however, it separately contracts a fraction of its total regulating power in a national auction. According to the documentation provided by the TSOs, the average contracted price for PFR in 2018 was 19.08 €/MW/h for the Netherlands and of 12.77 €/MW/h for the joint central European auction. In the U.K., a similar remuneration scheme is provided in the Phase 2 auction trial, an innovation project that procures frequency regulation products through the EPEX SPOT Auction Platform [38]. The auctions for the procuring of Dynamic Low High (DLH) frequency products, technically similar to PFR, saw an average price of 7.22 £/MW/h, which is significantly lower than the prices seen in Germany and the Netherlands.

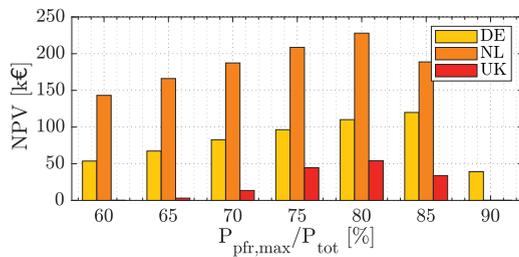
According to the investment cost and remuneration prices here discussed and summarized in Table IV, the Net Present Value (NPV) and break-even year of a BESS providing PFR in three case scenario have been evaluated. The NPV calculation was based on a time horizon of 25 years, compatible with the electrolytic capacitors and IGBT modules lifetime, as detailed in Section IV, and on a discount rate  $r$  of 2.5% [68]:

$$\text{NPV} = \sum_{t=1}^{25} \frac{R_t}{(1+r)^t} \quad (21)$$

**TABLE IV Economic Analysis Parameters**

Parameter	Value
Inflation rate	$r = 2.5\%$
Battery cost	330 €/kWh
PEC+BoP cost	150 €/kW
O&M costs	4.5 €/kWh/year
Average FCR price (NL) <sup>+</sup>	19.08 €/h/MW
Average PCR price (DE) <sup>+</sup>	12.77 €/h/MW
Average DLH price (UK) <sup>++</sup>	7.22 £/h/MW

<sup>+</sup> data extracted from [64], <sup>++</sup> data extracted from [38]



**FIG. 14. NPV over a 25 year project duration of a BESS systems rated 150 kW/150 kWh varying the fraction of the maximum power allocated for PFR,  $P_{pfr,max}$ .**

The yearly revenue parameter,  $R_t$ , reflects the income due to PFR provision, proportional to  $P_{pfr,max}$ , the percentage of the total power allocated for PFR, the investment and O&M costs, as detailed in Table IV, and the costs associated to the components replacements, where the replacement times are derived according to Section V.

The NPV is calculated for different  $P_{pfr,max}$  percentages. As already mentioned, the revenues deriving from PFR provisions are proportional to  $P_{pfr,max}$ , thus higher  $P_{pfr,max}$  gives higher revenues, however, components' wear increases as well, leading to earlier replacements of the BESS's components, as illustrated in Fig. 10 and Sections V. In Fig. 14, the NPV presents an optimal value, so a point where the system shows the highest profitability. However, comparing these optimal points, with the results of Fig. 10 and 13 it is possible to see that the  $P_{pfr,max}$  value that leads to the highest NPV is not necessarily the one that leads to the lowest components degradation. It is also clear that such functionality is profitable in each country, since it is possible to find a positive NPV. Furthermore, the case of the Netherlands leads to considerably higher revenues, with a maximum NPV 47% and 76% higher than in Germany and the U.K., due to the higher remuneration price [64].

## VII. CONCLUSION

This paper has analyzed the provision of PFR through BESSs in three case scenarios reflecting the technical and economic regulation of Germany, the U.K., and the Netherlands. The lifetime of the main BESS components subject to wear, the electrochemical storage, the IGBT modules, and the electrolytic capacitors have been investigated in different scenarios. As it has been illustrated in Section V, the component that is subject to faster degradation is the electrochemical

storage. Its lifetime peaks at 10-11 years, depending on the case scenario. The other two components whose lifetime has been investigated, electrolytic capacitors and IGBT modules, do not show significant wear due to the operation, when applied in BESS performing PFR, due to the very low power utilization of such functionality today. Nonetheless, the BESS lifetime estimation methodology can be applied for studying BESS lifetime when performing other functionalities.

Additionally, as detailed in the paper, the power sharing between the SoC management and PFR provision is a key variable for evaluating the BESS lifetime and the revenues deriving from the PFR provision. In this respect, it has been shown that the value of  $P_{pfr,max}$  that maximize the components lifetime does not necessarily coincide with the one that maximizes the BESS revenues.

Overall, the provision of PFR by means of BESS can be profitable in all the three countries analyzed, with the present remuneration tariffs and BESS capital costs. Furthermore, the higher remuneration tariffs seen in the Netherlands in recent years lead to the highest revenues between the analyzed countries.

Future work will focus on BESSs lifetime estimation and economic benchmark when deployed for performing other grid-connected services, such as the participation of energy markets, peak shaving and load, and services for the DSOs.

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